

ZXLD1366

High accuracy 1A, 60V LED driver with internal switch

Description

The ZXLD1366 is a continuous mode inductive step-down converter, designed for driving single or multiple series connected LEDs efficiently from a voltage source higher than the LED voltage. The device operates from an input supply between 6V and 60V and provides an externally adjustable output current of up to 1A. Depending upon supply voltage and external components, this can provide up to 48 watts of output power.

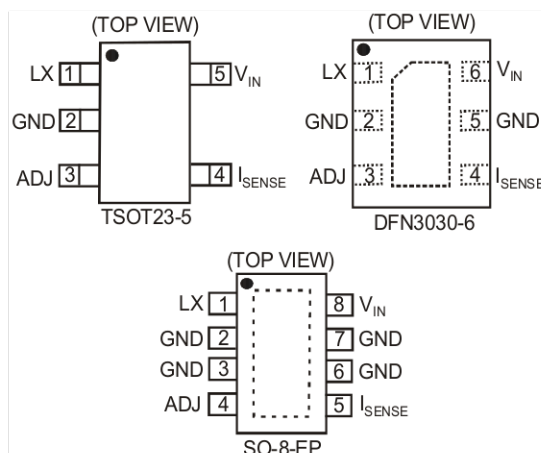
The ZXLD1366 includes the output switch and a high-side output current sensing circuit, which uses an external resistor to set the nominal average output current.

Output current can be adjusted above, or below the set value, by applying an external control signal to the 'ADJ' pin.

Features

- Typically better than 0.8% output current accuracy
- Available in thermally enhanced DFN package
- Simple and with low part count
- Single pin on/off and brightness control using DC voltage or PWM
- PWM resolution up to 1000:1
- High efficiency (up to 97%)
- Wide input voltage range: 6V to 60V
- Inherent open-circuit LED protection

Pin connections



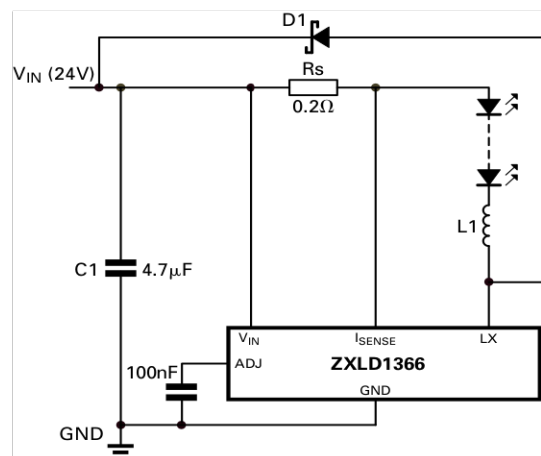
The ADJ pin will accept either a DC voltage or a PWM waveform. Depending upon the control frequency, this will provide either a continuous (dimmed) or a gated output current. Soft-start can be forced using an external capacitor from the ADJ pin to ground.

Applying a voltage of 0.2V or lower to the ADJ pin turns the output off and switches the device into a low current standby state.

Applications

- Low voltage halogen replacement LEDs
- Automotive lighting
- Low voltage industrial lighting
- LED back-up lighting
- Illuminated signs
- Emergency lighting
- SELV lighting
- LCD TV backlighting
- Refrigeration lights

Typical application circuit



Absolute maximum ratings (voltages to GND unless otherwise stated)

Input voltage (V_{IN})	-0.3V to +60V (65V for 0.5 sec)
I_{SENSE} voltage (V_{SENSE})	+0.3V to -5V (measured with respect to V_{IN})
LX output voltage (V_{LX})	-0.3V to +60V (65V for 0.5 sec)
Adjust pin input voltage (V_{ADJ})	-0.3V to +6V
Switch output current (I_{LX})	1.25A
Power dissipation (P_{tot})	SOT23-5; 1W: DFN; 1.8W
(Refer to package thermal de-rating curve on page 26)	
Operating temperature (T_{OP})	-40 to 125°C
Storage temperature (T_{ST})	-55 to 150°C
Junction temperature ($T_{j MAX}$)	150°C

These are stress ratings only. Operation outside the absolute maximum ratings may cause device failure. Operation at the absolute maximum ratings, for extended periods, may reduce device reliability.

Thermal resistance	TSOT23-5	SO-8-EP	DFN3030-6
Junction to ambient (Θ_{JA})	82°C/W	45°C/W	44°C/W
Junction to board (Ψ_{JB})	33°C/W	-	-
Junction to case (Θ_{JC})	-	7°C/W	14°C/W

Electrical characteristics (test conditions: $V_{IN}=24V$, $T_{amb}=25^{\circ}C$ unless otherwise stated)^(a)

Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
V_{IN}	Input voltage	See note ^(b)	6		60	V
V_{SU}	Internal regulator start-up threshold			4.85	5.2	V
V_{SD}	Internal regulator shutdown threshold		4.4	4.75		V
I_{INQoff}	Quiescent supply current with output off	ADJ pin grounded		65	108	μA
I_{INQon}	Quiescent supply current with output switching ^(c)	ADJ pin floating, L=68mH, 3 LEDs, f = 260kHz		1.6		mA
V_{SENSE}	Mean current sense threshold voltage (Defines LED current setting accuracy)	Measured on I_{SENSE} pin with respect to V_{IN} $V_{ADJ} = 1.25V$; $V_{IN}=18V$	195	200	205	μV
$V_{SENSEHYS}$	Sense threshold hysteresis			± 15		%
I_{SENSE}	I_{SENSE} pin input current	$V_{SENSE} = V_{IN} - 0.2$		4	10	μA
V_{REF}	Internal reference voltage	Measured on ADJ pin with pin floating		1.25		V
DV_{REF}/DT	Temperature coefficient of V_{REF}			50		ppm/°C
V_{ADJ}	External control voltage range on ADJ pin for DC brightness control ^(d)		0.3		2.5	V
V_{ADJoff}	DC voltage on ADJ pin to switch device from active (on) state to quiescent (off) state	V_{ADJ} falling	0.15	0.2	0.27	V

NOTES:

- (a) Production testing of the device is performed at 25°C. Functional operation of the device and parameters specified over a -40°C to +105°C temperature range, are guaranteed by design, characterization and process control.
- (b) $V_{IN} > 16V$ to fully enhance output transistor. Otherwise out current must be derated - see graphs. Operation at low supply may cause excessive heating due to increased on-resistance. Tested at 7V guaranteed for 6V by design.
- (c) Static current of device is approximately 700 mA, see Graph, Page 17
- (d) 100% brightness corresponds to $V_{ADJ} = V_{ADJ(nom)} = V_{REF}$. Driving the ADJ pin above V_{REF} will increase the V_{SENSE} threshold and output current proportionally.

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Electrical characteristics (test conditions: $V_{IN}=24V$, $T_{amb}=25^{\circ}C$ unless otherwise stated) (cont.)

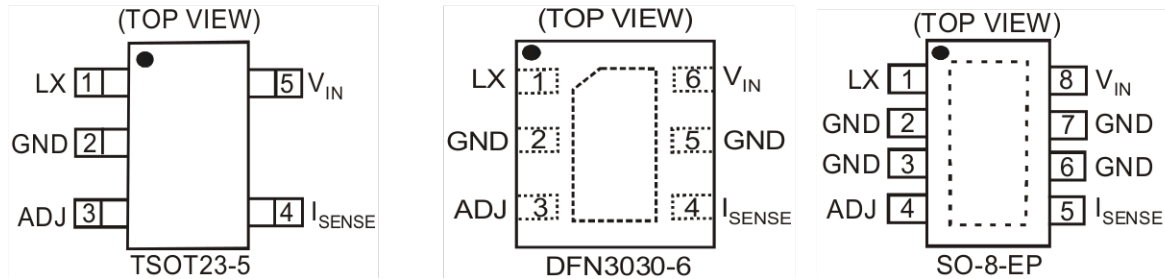
Symbol	Parameter	Conditions	Min.	Typ.	Max.	Unit
$V_{ADJ_{on}}$	DC voltage on ADJ pin to switch device from quiescent (off) state to active (on) state	V_{ADJ} rising	0.2	0.25	0.3	V
R_{ADJ}	Resistance between ADJ pin and V_{REF}	$0 < V_{ADJ} < V_{REF}$ $V_{ADJ} > V_{REF} + 100mV$	30 10.4	50 14.2	65 18	k Ω k Ω
$I_{LX_{mean}}$	Continuous LX switch current				1	A
R_{LX}	LX Switch 'On' resistance	@ $I_{LX} = 1 A$		0.5	0.75	Ω
$I_{LX(leak)}$	LX switch leakage current				5	μA
$D_{PWM(LF)}$	Duty cycle range of PWM signal applied to ADJ pin during low frequency PWM dimming mode Brightness control range	PWM frequency <300Hz PWM amplitude = V_{REF} Measured on ADJ pin	0.001		1	
$DC_{ADJ}^{(*)}$	DC Brightness control range	See note (*)		5:1		
T_{SS}	Soft start time	Time taken for output current to reach 90% of final value after voltage on ADJ pin has risen above 0.3V Requires external capacitor 22nF. See graphs for more details		2		ms
f_{LX}	Operating frequency (See graphs for more detail)	ADJ pin floating $L = 68mH (0.2V)$ $I_{OUT} = 1A @ V_{LED} = 3.6V$ Driving 3 LEDs		260		kHz
T_{ONmin}	Minimum switch 'ON' time	LX switch 'ON'		130 (†)		ns
T_{OFFmin}	Minimum switch 'OFF' time	LX switch 'OFF'		70 (†)		ns
T_{PWmin_REC}	Recommended minimum switch pulse width	LX switch 'ON' or 'OFF'		800		ns
f_{LXmax}	Recommended maximum operating frequency				500	kHz
D_{LX}	Recommended duty cycle range of output switch at f_{LXmax}		0.3		0.7	

NOTES:

(*) Ratio of maximum brightness to minimum brightness before shutdown $V_{REF} = 1.25/0.3$. V_{REF} externally driven to 2.5V, ratio 10:1.

(†) Parameters are not tested at production. Parameters are guaranteed by design, characterization and process control.

Pin description



Name	TSOT23-5	DFN3030-6	SO8-EP	Description
LX	1	1	1	Drain of NDMOS switch
GND	2	2, 5	2, 3, 6, 7	Ground (0V)
ADJ	3	3	4	Multi-function On/Off and brightness control pin: <ul style="list-style-type: none"> • Leave floating for normal operation. ($V_{ADJ} = V_{REF} = 1.25V$ giving nominal average output current $I_{OUTnom} = 0.2V/R_S$) • Drive to voltage below 0.2V to turn off output current • Drive with DC voltage ($0.3V < V_{ADJ} < 2.5V$) to adjust output current from 25% to 200% of I_{OUTnom} • Connect a capacitor from this pin to ground to set soft-start time. Soft start time increases approximately 0.2ms/nF
I _{SENSE}	4	4	5	Connect resistor R_S from this pin to V_{IN} to define nominal average output current $I_{OUTnom} = 0.2V/R_S$ (Note: $R_{SMIN} = 0.2V$ with ADJ pin open-circuit)
V _{IN}	5	6	8	Input voltage (6V to 60V). Decouple to ground with 4.7mF or higher X7R ceramic capacitor close to device
Tab	N/A	Tab	Tab	Not internally connected. Connect to ground plane to improve thermal efficiency

Ordering information

Device	Package	Reel size (inches)	Reel width (mm)	Quantity per reel	Device Mark
ZXLD1366ET5TA	TSOT23-5	7"	8	3,000	1366
ZXLD1366DACTC	DFN3030-6	13"	12	3,000	1366
ZXLD1366EN8TC	SO-8-EP	13"	12"	2,500	1366

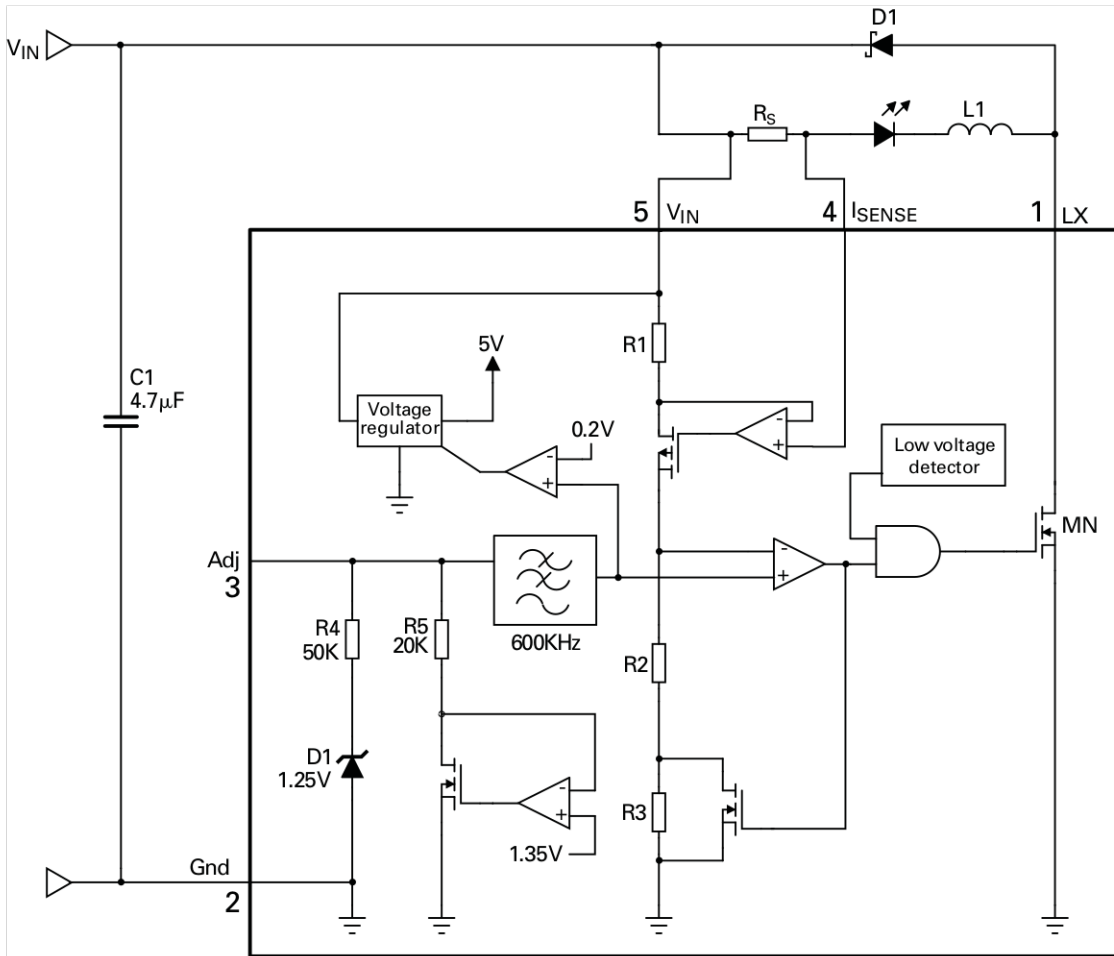


Figure 1 Block diagram - Pin connection for TSOT23-5 package

Device description

The device, in conjunction with the coil (L1) and current sense resistor (R_S), forms a self-oscillating continuous-mode buck converter.

Device operation (refer to Figure 1 - Block diagram and Figure 2 Operating waveforms)

Operation can be best understood by assuming that the ADJ pin of the device is unconnected and the voltage on this pin (V_{ADJ}) appears directly at the (+) input of the comparator.

When input voltage V_{IN} is first applied, the initial current in L1 and R_S is zero and there is no output from the current sense circuit. Under this condition, the (-) input to the comparator is at ground and its output is high. This turns MN on and switches the LX pin low, causing current to flow from V_{IN} to ground, via R_S , L1 and the LED(s). The current rises at a rate determined by V_{IN} and L1 to produce a voltage ramp (V_{SENSE}) across R_S . The supply referred voltage V_{SENSE} is forced across internal resistor R1 by the current sense circuit and produces a proportional current in internal resistors R2 and R3. This produces a ground referred rising voltage at the (-) input of the comparator. When this reaches the threshold voltage (V_{ADJ}), the comparator output switches low and MN turns off. The comparator output also drives another NMOS switch, which bypasses internal resistor R3 to provide a controlled amount of hysteresis. The hysteresis is set by R3 to be nominally 15% of V_{ADJ} .

When MN is off, the current in L1 continues to flow via D1 and the LED(s) back to V_{IN} . The current decays at a rate determined by the LED(s) and diode forward voltages to produce a falling voltage at the input of the comparator. When this voltage returns to V_{ADJ} , the comparator output switches high again. This cycle of events repeats, with the comparator input ramping between limits of $V_{ADJ} \pm 15\%$.

Switching thresholds

With $V_{ADJ} = V_{REF}$, the ratios of R1, R2 and R3 define an average V_{SENSE} switching threshold of 200mV (measured on the I_{SENSE} pin with respect to V_{IN}). The average output current I_{OUTnom} is then defined by this voltage and R_S according to:

$$I_{OUTnom} = 200mV/R_S$$

Nominal ripple current is $\pm 30mV/R_S$

Adjusting output current

The device contains a low pass filter between the ADJ pin and the threshold comparator and an internal current limiting resistor (50k Ω nom) between ADJ and the internal reference voltage. This allows the ADJ pin to be overdriven with either DC or pulse signals to change the V_{SENSE} switching threshold and adjust the output current.

Details of the different modes of adjusting output current are given in the applications section.

Output shutdown

The output of the low pass filter drives the shutdown circuit. When the input voltage to this circuit falls below the threshold (0.2V nom.), the internal regulator and the output switch are turned off. The voltage reference remains powered during shutdown to provide the bias current for the shutdown circuit. Quiescent supply current during shutdown is nominally 60 μ A and switch leakage is below 5 μ A.

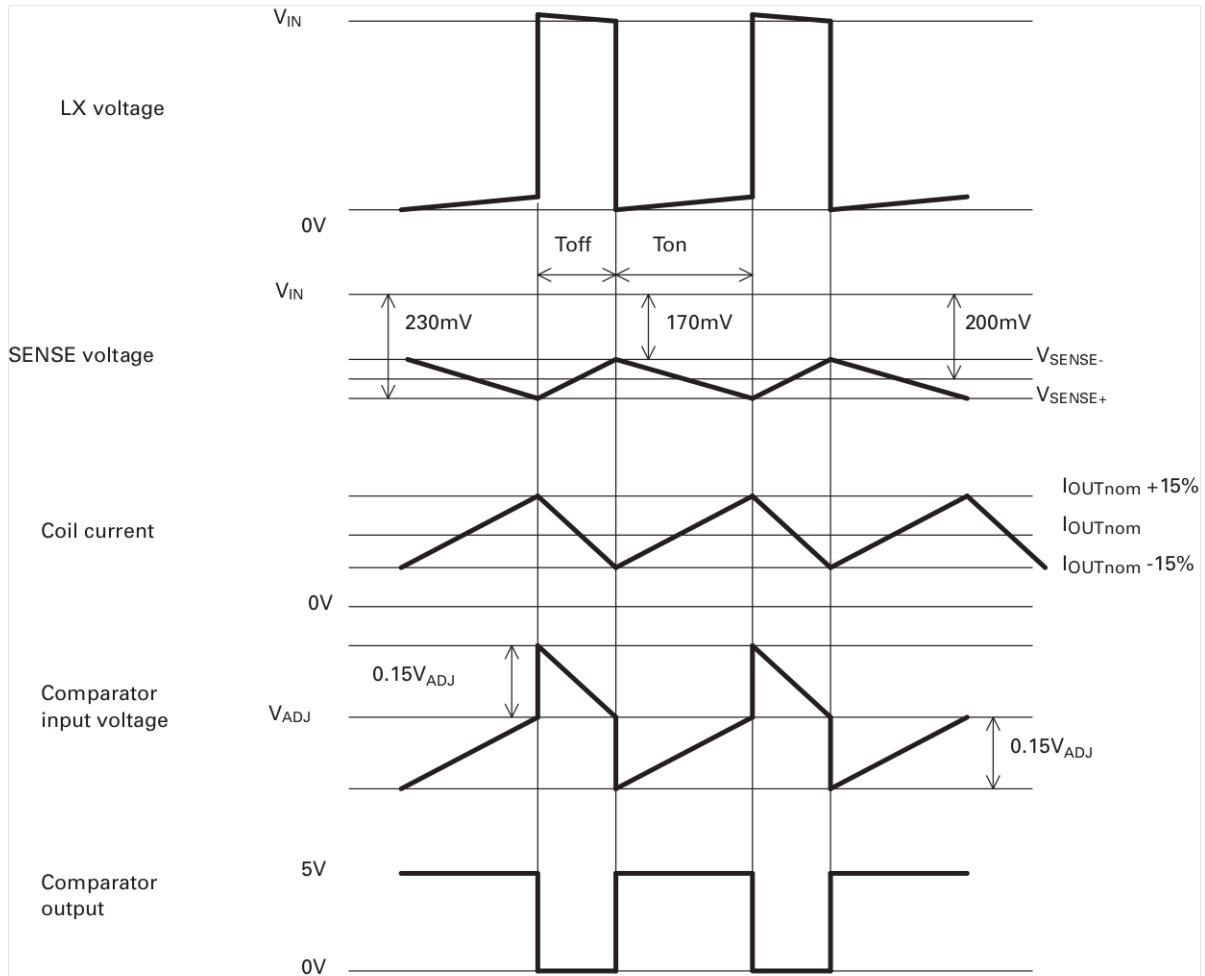
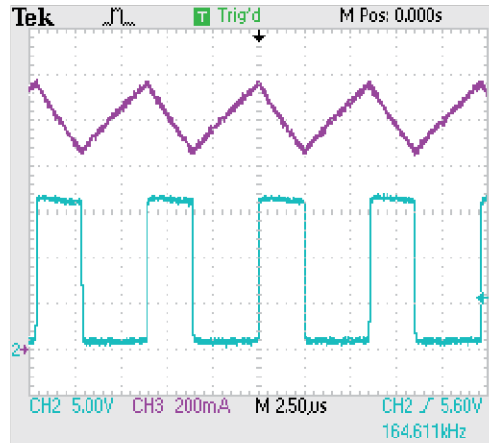


Figure 2 Theoretical operating waveforms

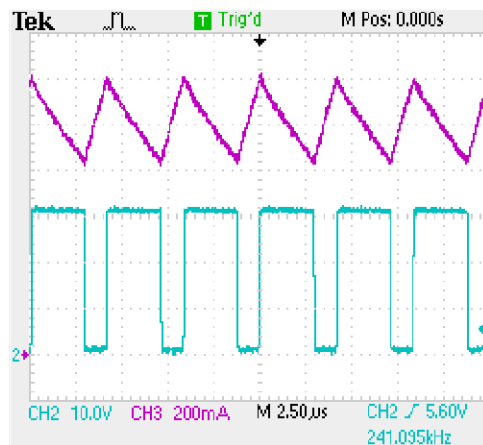
Actual operating waveforms [$V_{IN}=15V$, $R_S=0.2V$, $L=68\mu H$]

Normal operation. Output current (Ch3) and LX voltage (Ch2)



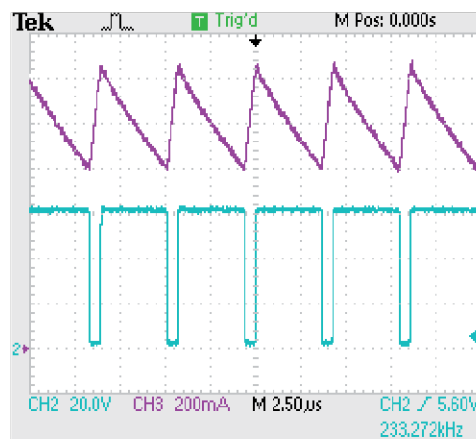
Actual operating waveforms [$V_{IN}=30V$, $R_S=0.2V$, $L=68\mu H$]

Normal operation. Output current (Ch3) and LX voltage (Ch2)



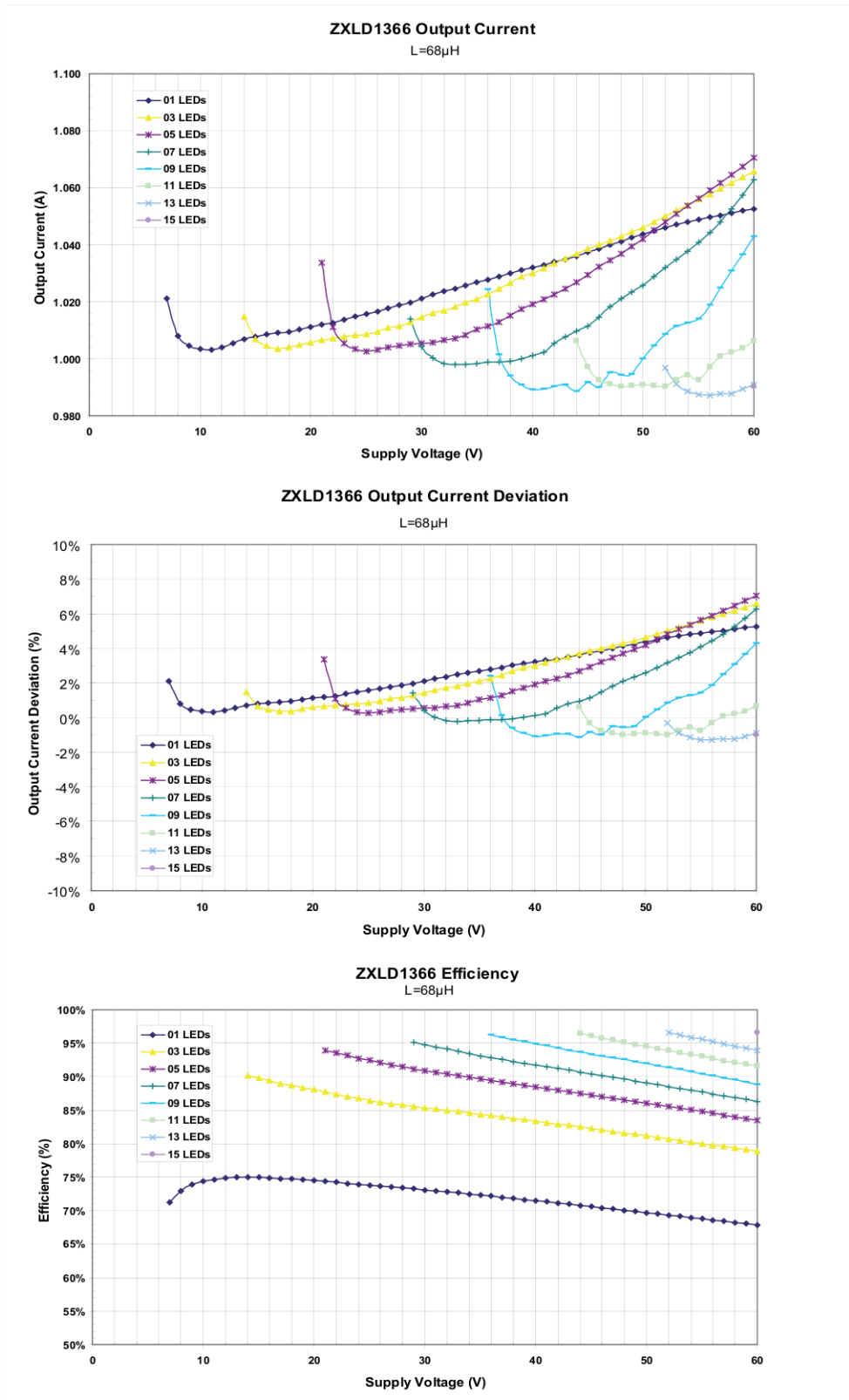
Actual operating waveforms [$V_{IN}=60V$, $R_S=0.2V$, $L=68\mu H$]

Normal operation. Output current (Ch3) and LX voltage (Ch2)

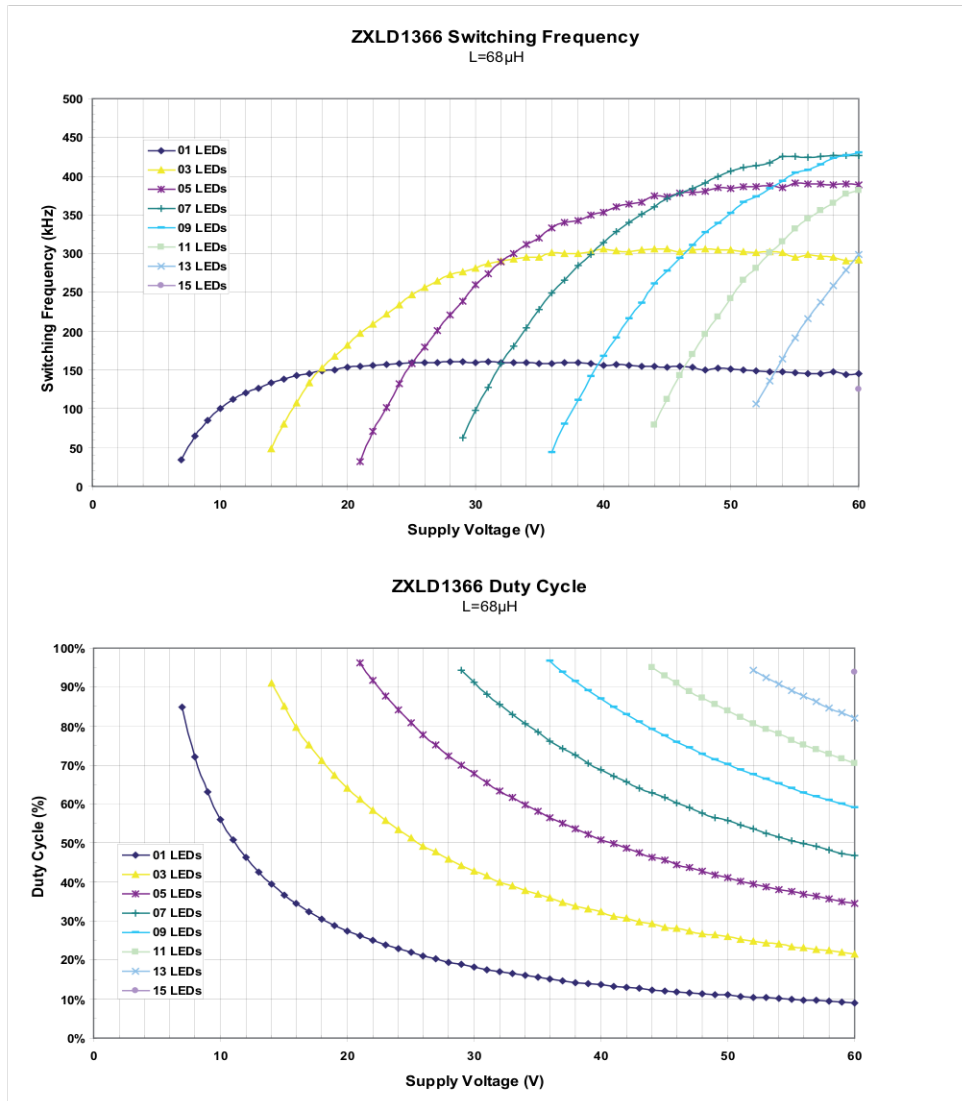


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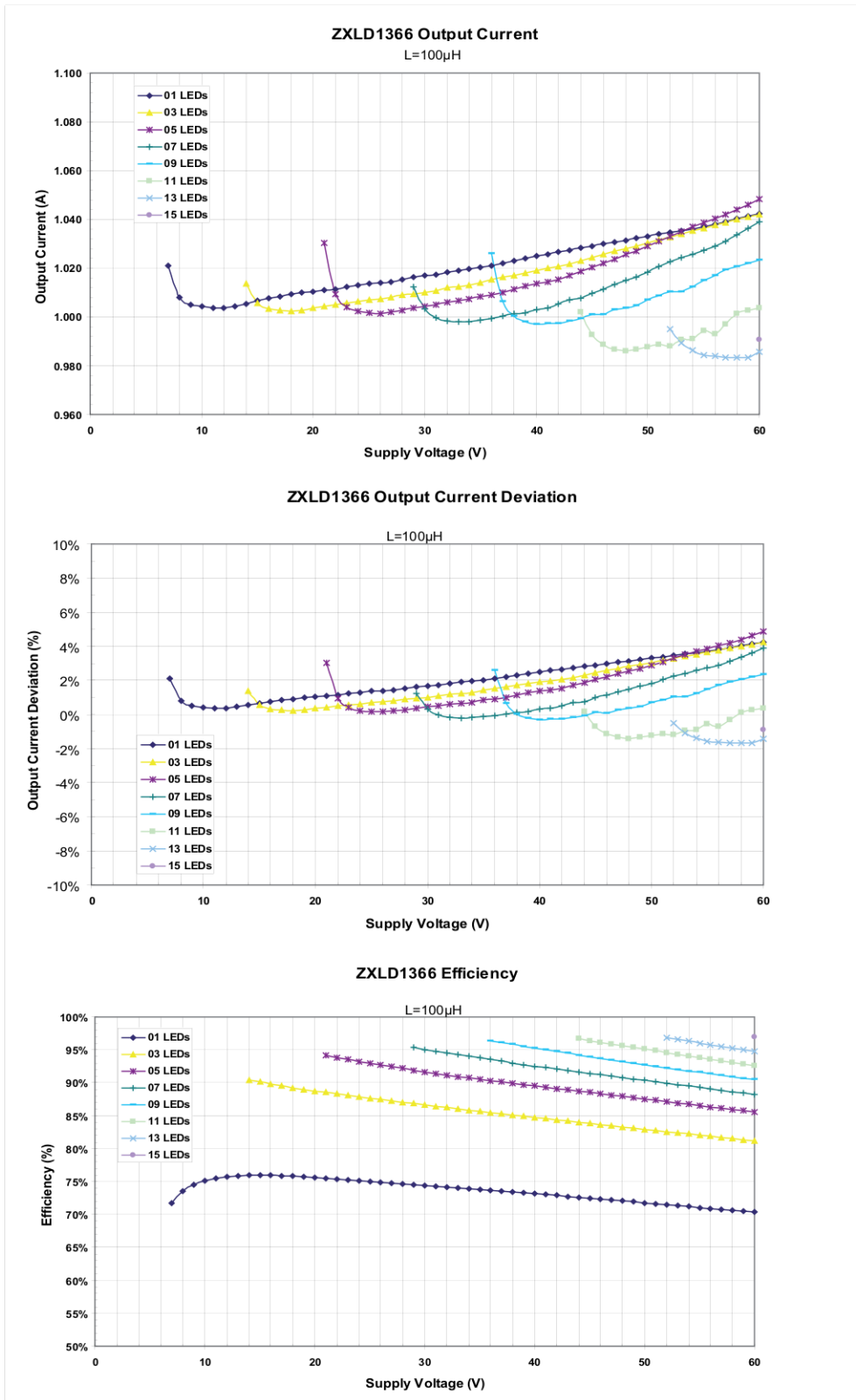
Typical operating conditions



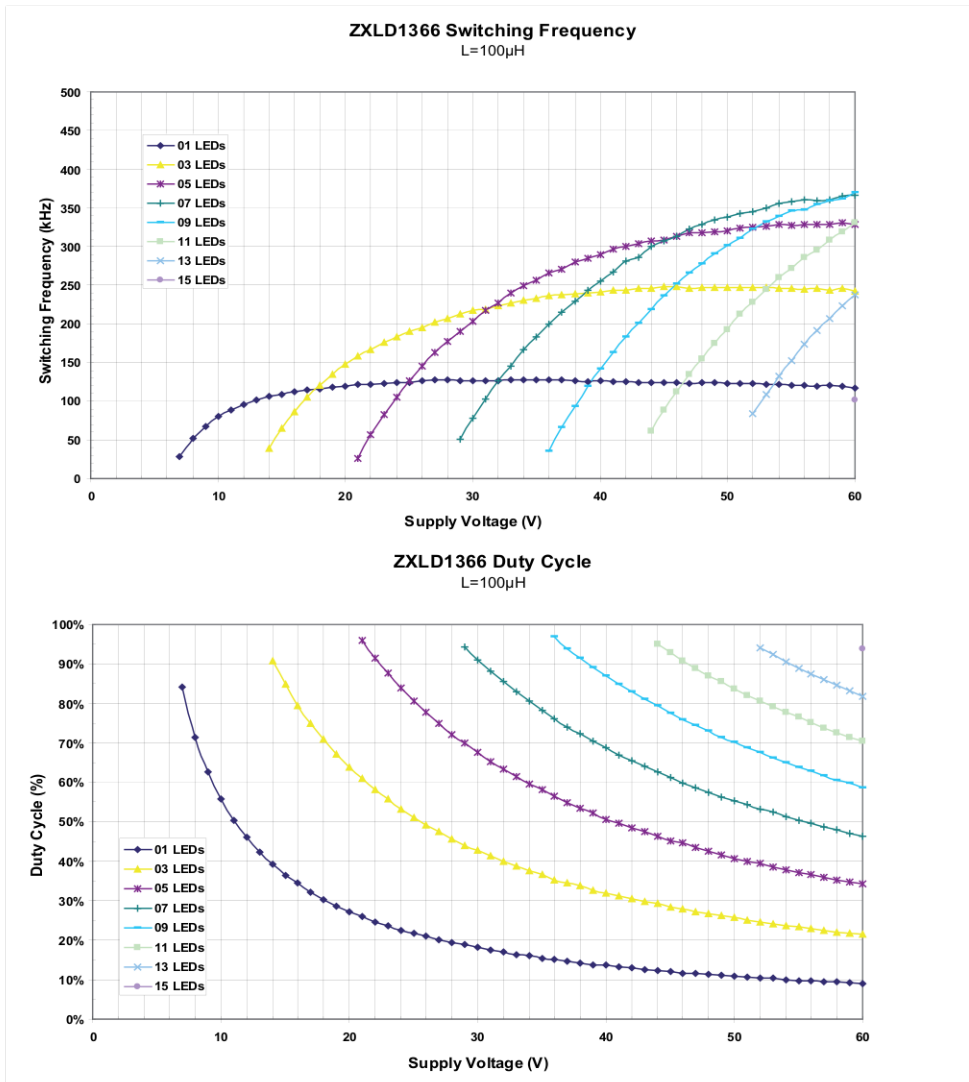
Typical operating conditions



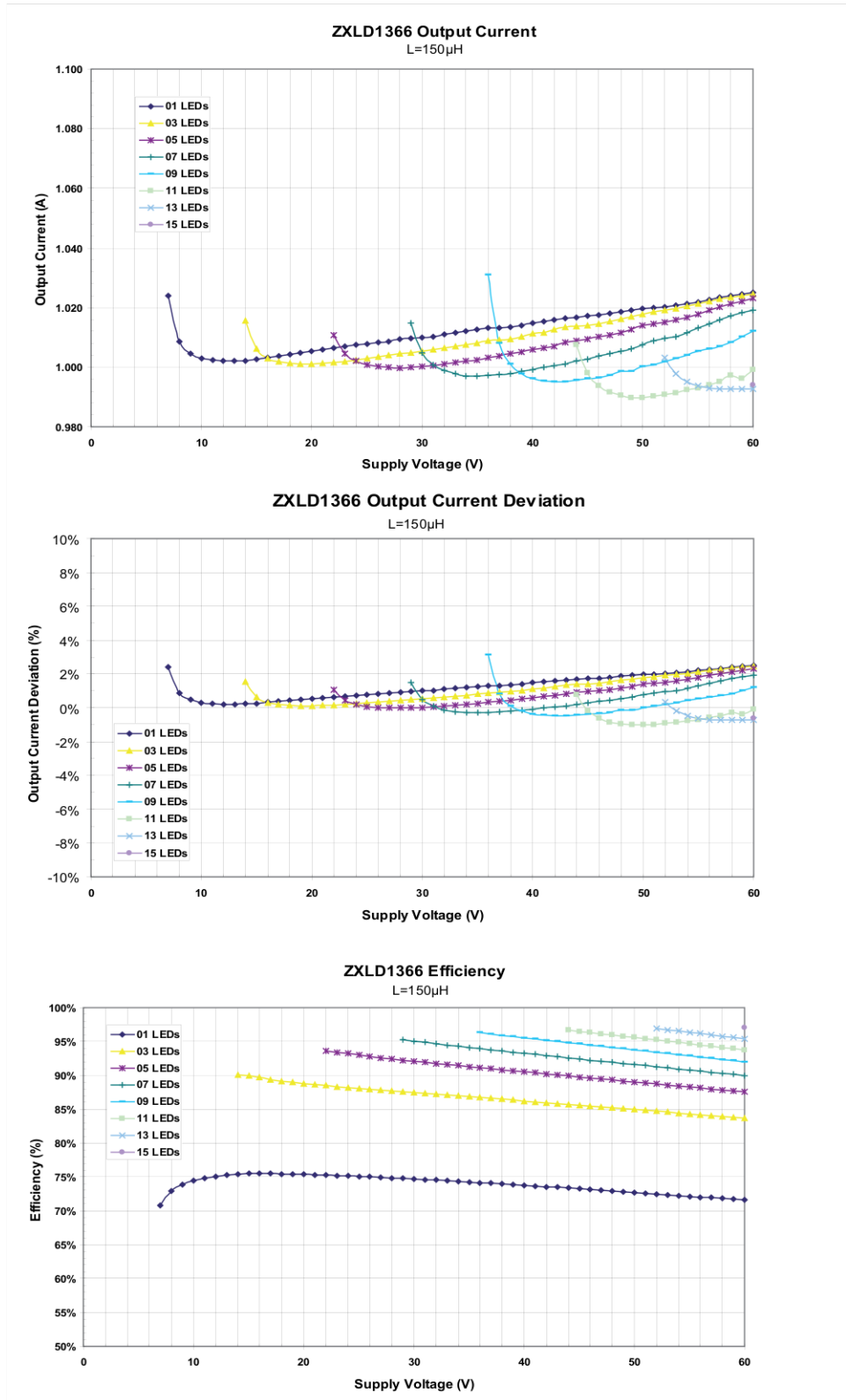
Typical operating conditions



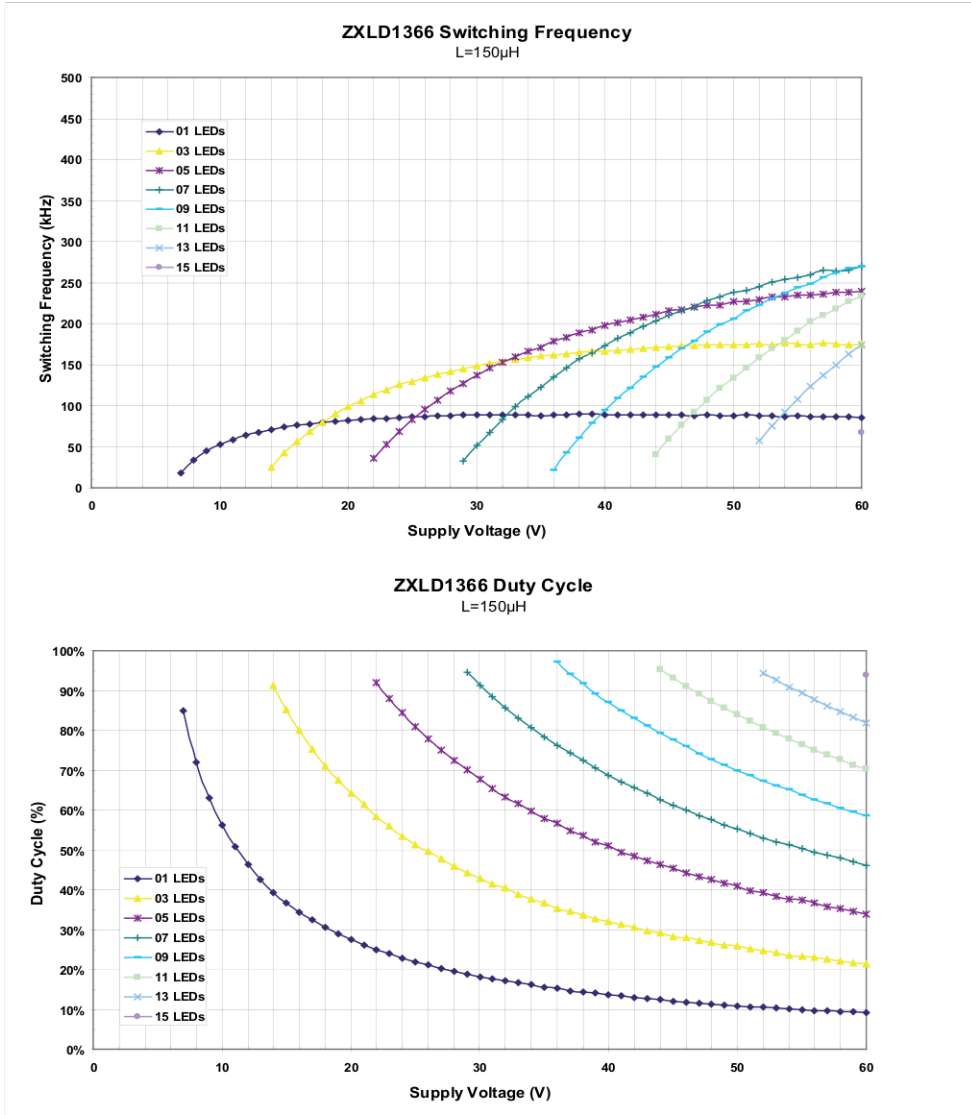
Typical operating conditions



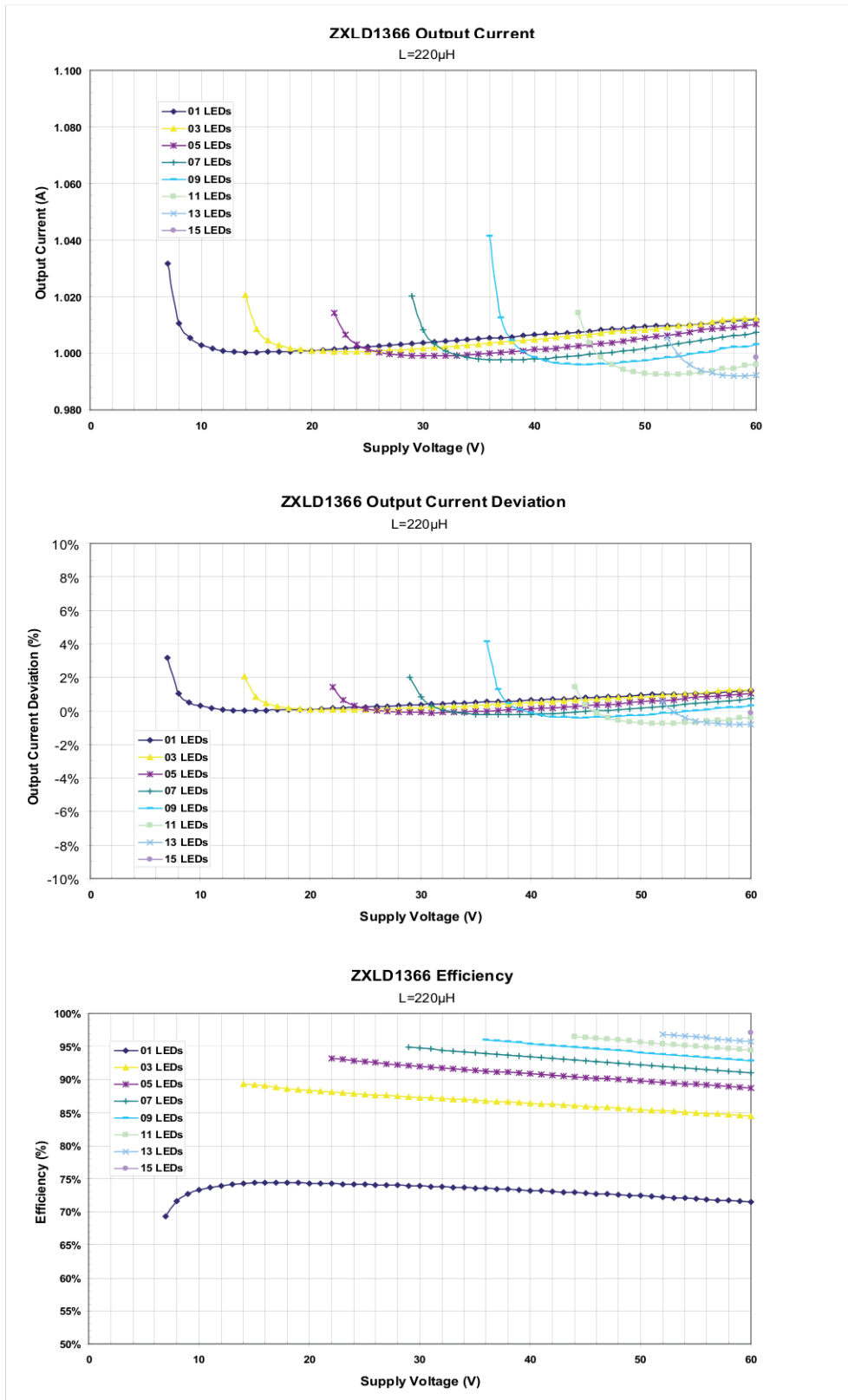
Typical operating conditions



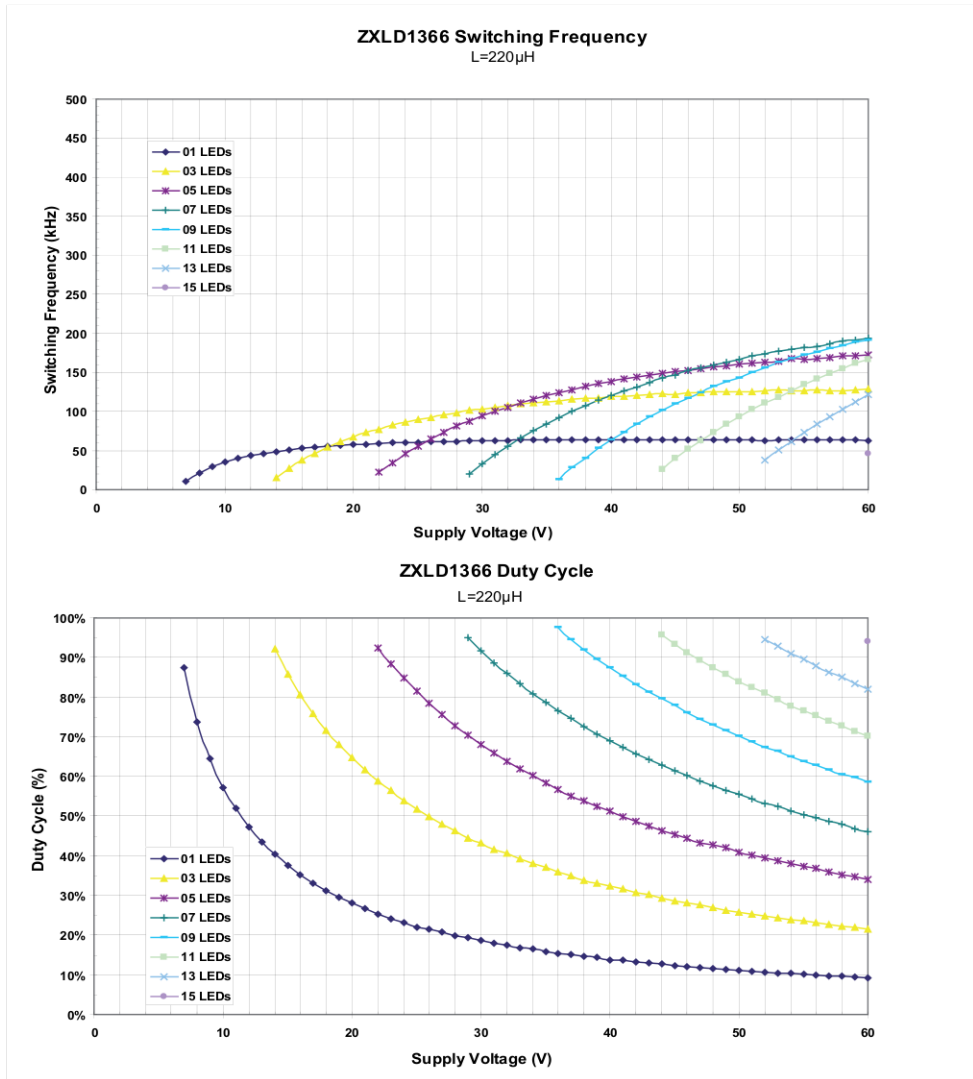
Typical operating conditions



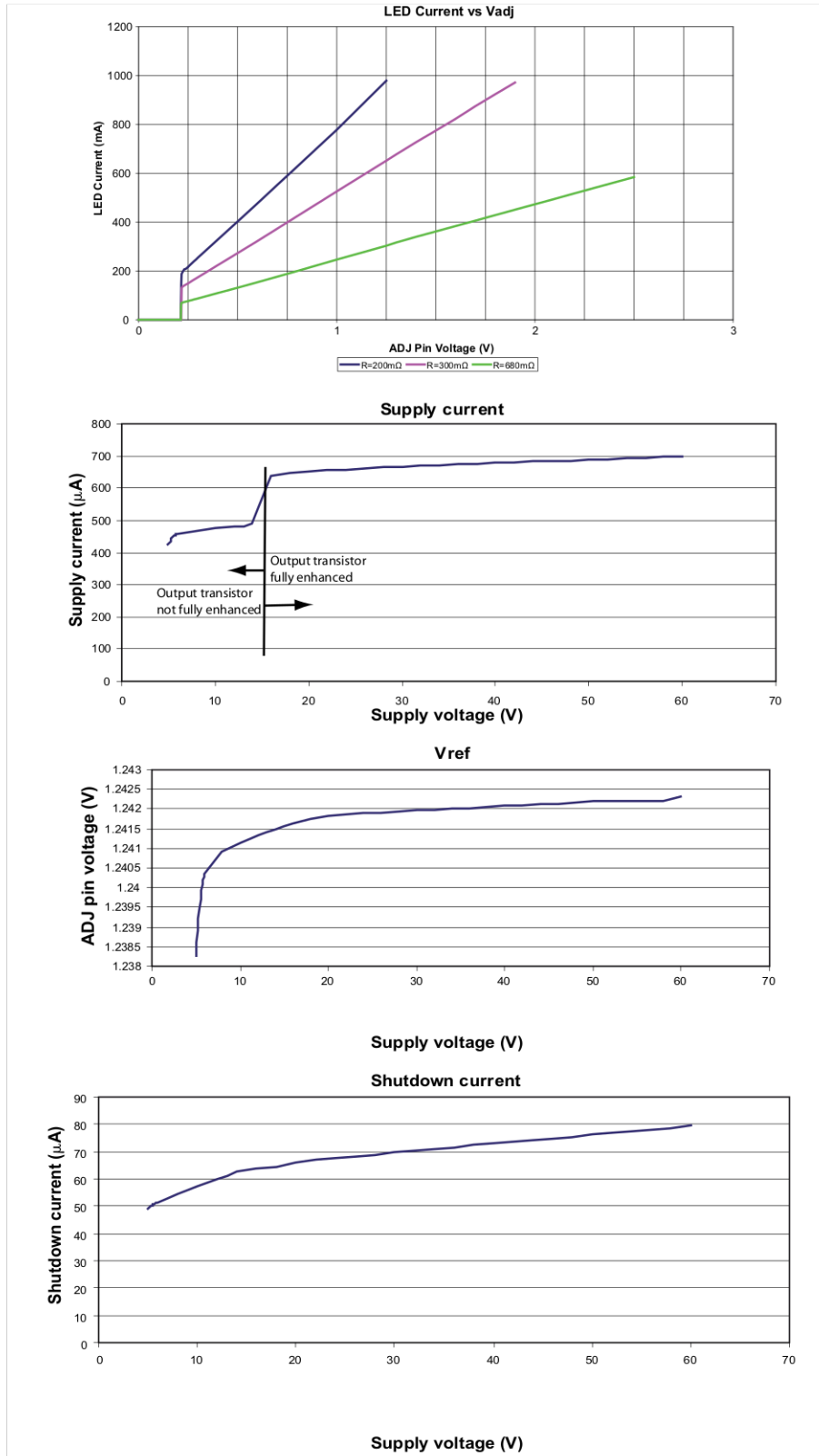
Typical operating conditions



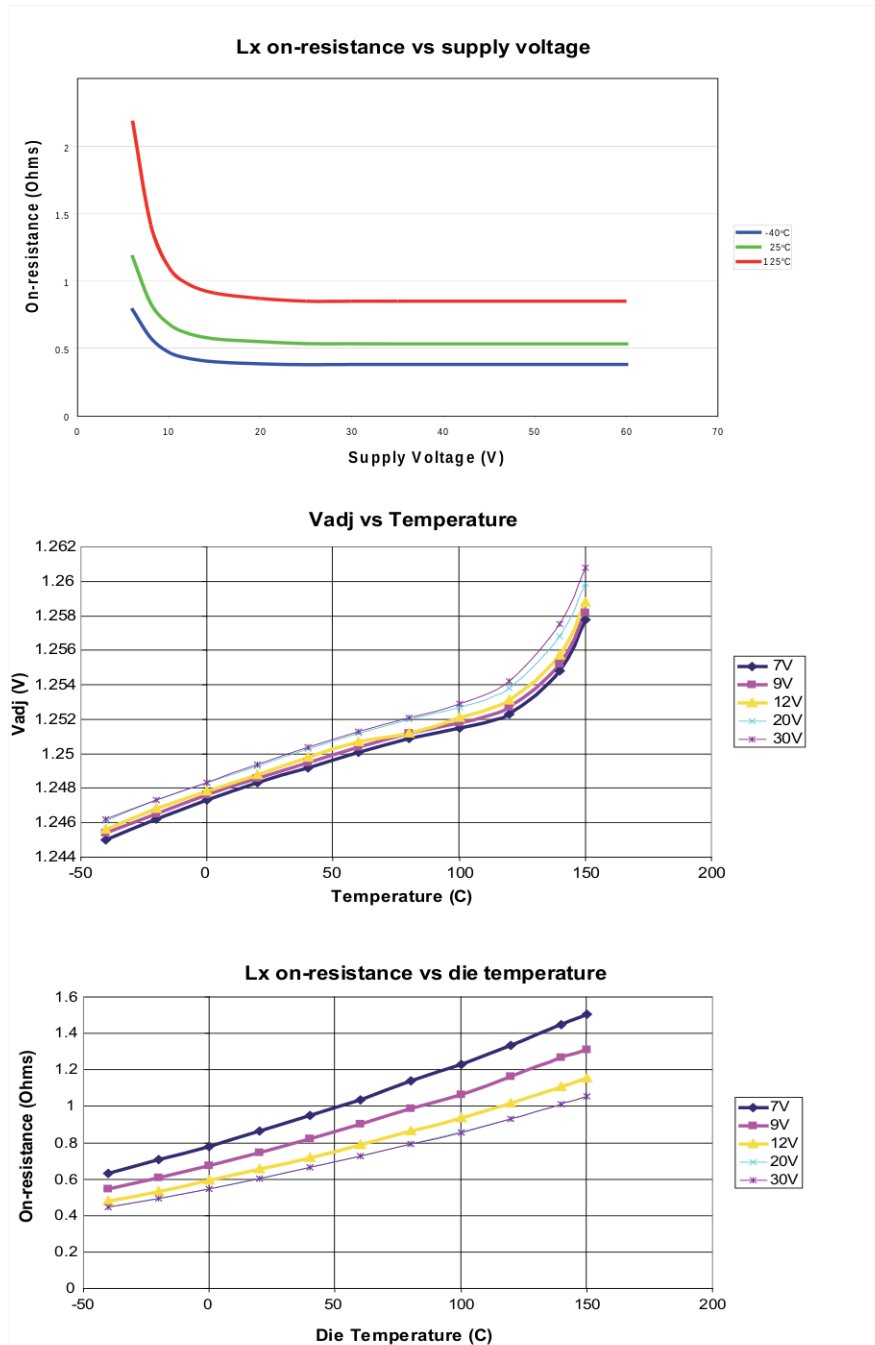
Typical operating conditions



Typical operating conditions



Typical operating conditions



Application information

Setting nominal average output current with external resistor RS

The nominal average output current in the LED(s) is determined by the value of the external current sense resistor (R_S) connected between V_{IN} and I_{SENSE} and is given by:

$$I_{OUTnom} = 0.2/R_S \text{ [for } R_S \geq 0.2V\text{]}$$

The table below gives values of nominal average output current for several preferred values of current setting resistor (R_S) in the typical application circuit shown on page 1:

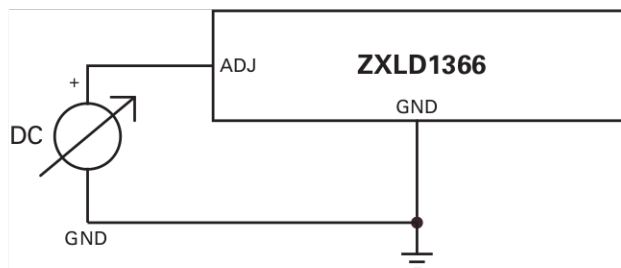
R_S (V)	Nominal average output current (mA)
0.20	1000
0.27	740
0.56	357

The above values assume that the ADJ pin is floating and at a nominal voltage of V_{REF} ($=1.25V$). Note that $R_S = 0.2V$ is the minimum allowed value of sense resistor under these conditions to maintain switch current below the specified maximum value.

It is possible to use different values of R_S if the ADJ pin is driven from an external voltage. (See next section).

Output current adjustment by external DC control voltage

The ADJ pin can be driven by an external dc voltage (V_{ADJ}), as shown, to adjust the output current to a value above or below the nominal average value defined by R_S .



The nominal average output current in this case is given by:

$$I_{OUTdc} = (V_{ADJ} / 1.25) \times (0.2/R_S) \text{ [for } 0.3 < V_{ADJ} < 2.5V\text{]}$$

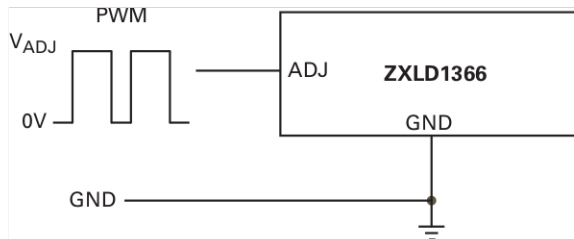
Note that 100% brightness setting corresponds to $V_{ADJ} = V_{REF}$. When driving the ADJ pin above 1.25V, R_S must be increased in proportion to prevent I_{OUTdc} exceeding 1A maximum.

The input impedance of the ADJ pin is $50k\Omega \pm 25\%$ for voltages below V_{REF} and $14.2k\Omega \pm 25\%$ for voltages above $V_{REF} + 100mV$.

Output current adjustment by PWM control

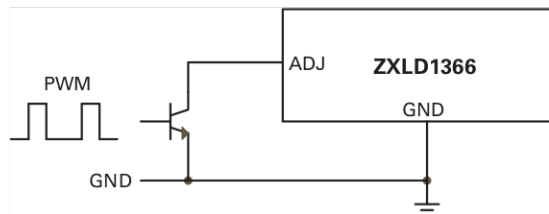
Directly driving ADJ input

A Pulse Width Modulated (PWM) signal with duty cycle D_{PWM} can be applied to the ADJ pin, as shown below, to adjust the output current to a value above or below the nominal average value set by resistor R_S :



Driving the ADJ input via open collector transistor

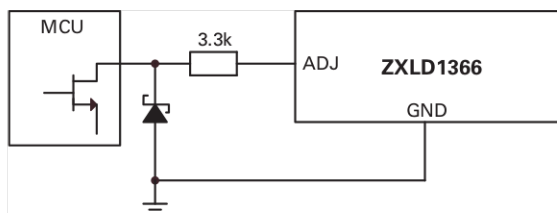
The recommended method of driving the ADJ pin and controlling the amplitude of the PWM waveform is to use a small NPN switching transistor as shown below:



This scheme uses the 50k resistor between the ADJ pin and the internal voltage reference as a pull-up resistor for the external transistor.

Driving the ADJ input from a microcontroller

Another possibility is to drive the device from the open drain output of a microcontroller. The diagram below shows one method of doing this:



If the NMOS transistor within the microcontroller has high Gate / Drain capacitance, this arrangement can inject a negative spike into ADJ input of the ZXLD1366 and cause erratic operation but the addition of a Schottky clamp diode (eg Diodes Inc. SD103CWS) to ground and inclusion of a series resistor (3.3k) will prevent this. See the section on PWM dimming for more details of the various modes of control using high frequency and low frequency PWM signals.

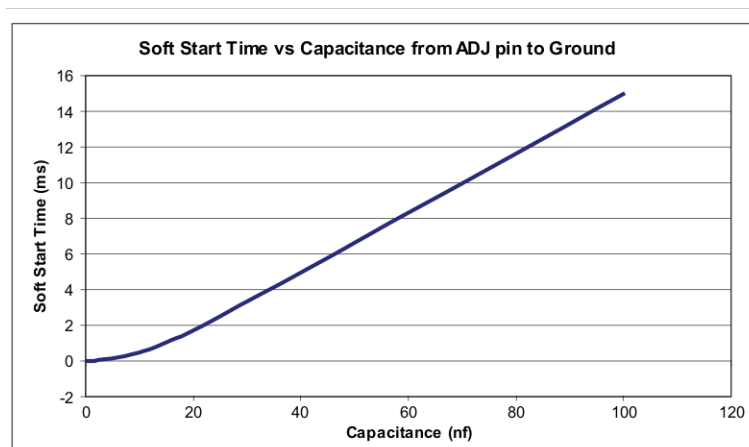
Shutdown mode

Taking the ADJ pin to a voltage below 0.2V for more than approximately 100 μ s will turn off the output and supply current to a low standby level of 65 μ A nominal.

Note that the ADJ pin is not a logic input. Taking the ADJ pin to a voltage above V_{REF} will increase output current above the 100% nominal average value. (See page 18 graphs for details).

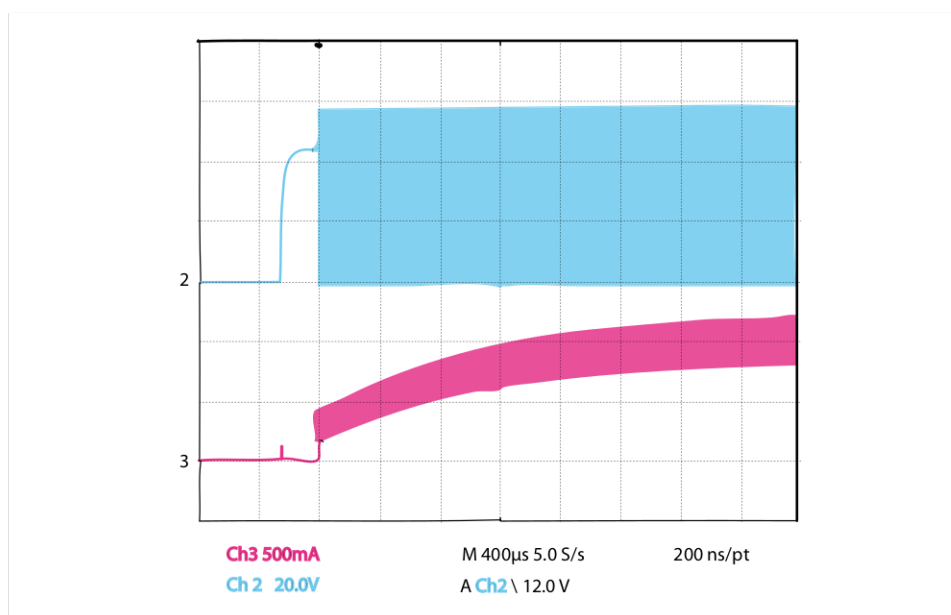
Soft-start

An external capacitor from the ADJ pin to ground will provide a soft-start delay, by increasing the time taken for the voltage on this pin to rise to the turn-on threshold and by slowing down the rate of rise of the control voltage at the input of the comparator. Adding capacitance increases this delay by approximately 0.2ms/nF. The graph below shows the variation of soft-start time for different values of capacitor.



Actual operating waveforms [$V_{IN}=60V$, $R_S=0.2V$, $L=68\mu H$, 22nF on ADJ]

Soft-start operation. LX voltage (CH2) and Output current (CH3) using a 22nF external capacitor on the ADJ pin.



V_{IN} capacitor selection

A low ESR capacitor should be used for input decoupling, as the ESR of this capacitor appears in series with the supply source impedance and lowers overall efficiency. This capacitor has to supply the relatively high peak current to the coil and smooth the current ripple on the input supply.

To avoid transients into the IC, the size of the input capacitor will depend on the V_{IN} voltage:

$$V_{IN} = 6 \text{ to } 40\text{V} \quad C_{IN} = 2.2\mu\text{F}$$

$$V_{IN} = 40 \text{ to } 50\text{V} \quad C_{IN} = 4.7\mu\text{F}$$

$$V_{IN} = 50 \text{ to } 60\text{V} \quad C_{IN} = 10\mu\text{F}$$

When the input voltage is close to the output voltage the input current increases which puts more demand on the input capacitor. The minimum value of $2.2\mu\text{F}$ may need to be increased to $4.7\mu\text{F}$; higher values will improve performance at lower input voltages, especially when the source impedance is high. The input capacitor should be placed as close as possible to the IC.

For maximum stability over temperature and voltage, capacitors with X7R, X5R, or better dielectric is recommended. Capacitors with Y5V dielectric are not suitable for decoupling in this application and should **NOT** be used.

When higher voltages are used with the $C_{IN} = 10\mu\text{F}$, an electrolytic capacitor can be used provided that a suitable 1mF ceramic capacitor is also used and positioned as close to the V_{IN} pin as possible.

A suitable capacitor would be NACEW100M1006.3x8TR13F (NIC Components).

The following web sites are useful when finding alternatives:

www.murata.com

www.niccomp.com

www.kemet.com

Inductor selection

Recommended inductor values for the ZXLD1366 are in the range 68 μH to 220 μH .

Higher values of inductance are recommended at higher supply voltages in order to minimize errors due to switching delays, which result in increased ripple and lower efficiency. Higher values of inductance also result in a smaller change in output current over the supply voltage range. (see graphs pages 10-17). The inductor should be mounted as close to the device as possible with low resistance connections to the LX and V_{IN} pins.

The chosen coil should have a saturation current higher than the peak output current and a continuous current rating above the required mean output current.

Suitable coils for use with the ZXLD1366 may be selected from the MSS range manufactured by Coilcraft, or the NPIS range manufactured by NIC components. The following websites may be useful in finding suitable components

www.coilcraft.com

www.niccomp.com

www.wuerth-elektronik.de

The inductor value should be chosen to maintain operating duty cycle and switch 'on'/'off' times within the specified limits over the supply voltage and load current range.

The graph Figure 3 below can be used to select a recommended inductor based on maintaining the ZXLD1366 case temperature below 60°C. For detailed performance characteristics for the inductor values 68, 100, 150 and 220 μH see graphs on pages 10-17.

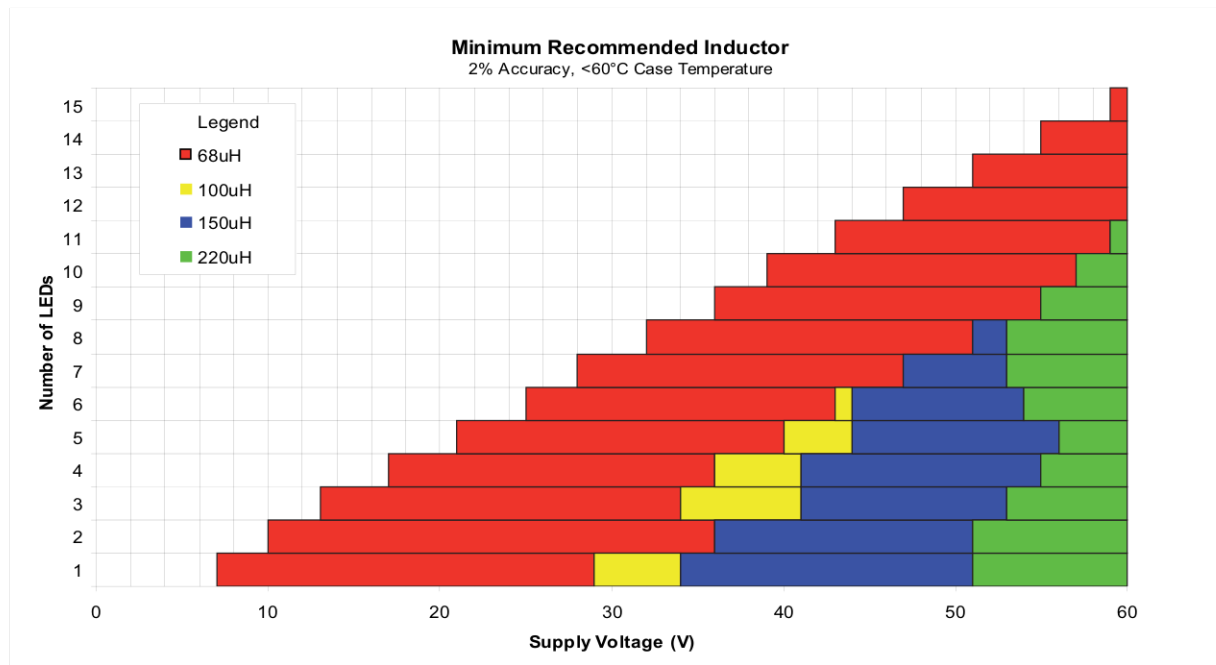


Figure 3 ZXLD1366 Minimum recommended inductor (TSOT23-5)

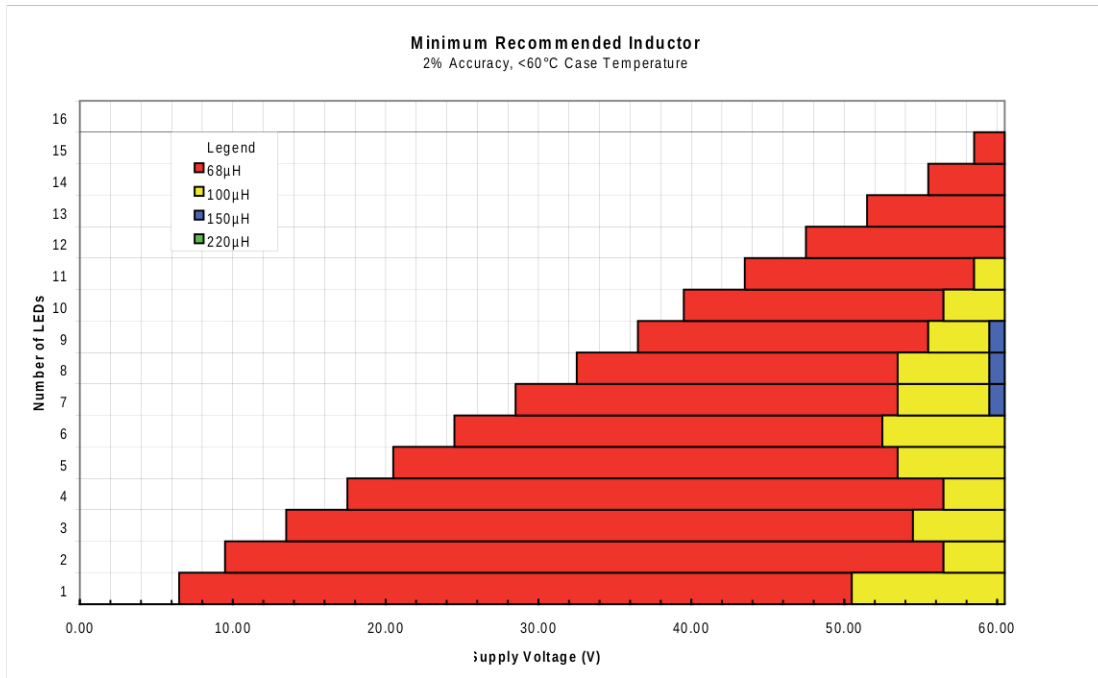


Figure 4 ZXLD1366 Minimum recommended inductor (DFN3030-6)

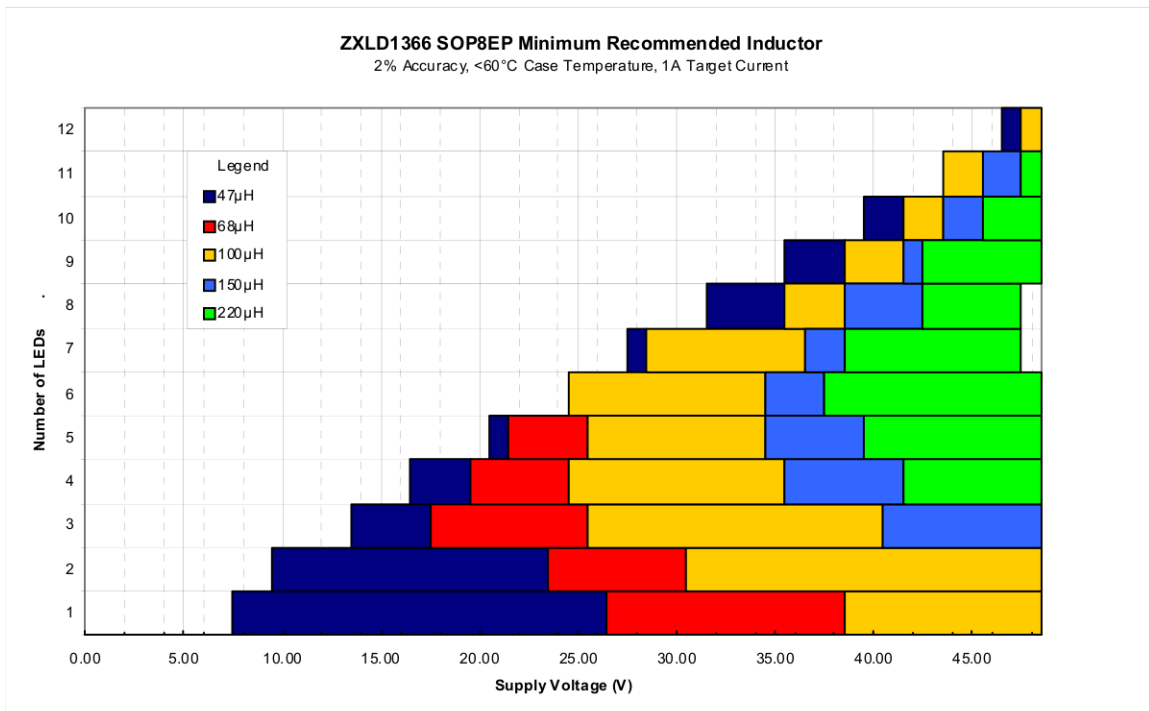


Figure 5 ZXLD1366 Minimum recommended inductor (SO-8-EP)

Diode Selection

For maximum efficiency and performance, the rectifier (D1) should be a fast low capacitance Schottky diode* with low reverse leakage at the maximum operating voltage and temperature.

They also provide better efficiency than silicon diodes, due to a combination of lower forward voltage and reduced recovery time.

It is important to select parts with a peak current rating above the peak coil current and a continuous current rating higher than the maximum output load current. It is very important to consider the reverse leakage of the diode when operating above 85°C. Excess leakage will increase the power dissipation in the device and if close to the load may create a thermal runaway condition.

The higher forward voltage and overshoot due to reverse recovery time in silicon diodes will increase the peak voltage on the LX output. If a silicon diode is used, care should be taken to ensure that the total voltage appearing on the LX pin including supply ripple, does not exceed the specified maximum value.

*A suitable Schottky diode would be B3100 (Diodes Inc).

Reducing output ripple

Peak to peak ripple current in the LED(s) can be reduced, if required, by shunting a capacitor C_{led} across the LED(s) as shown below:

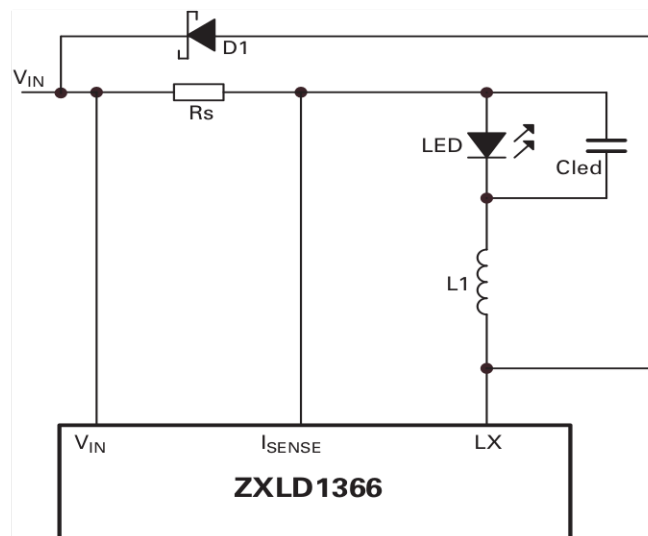


Figure 6 Reduce Output Ripple

A value of 1 mF will reduce the supply ripple current by a factor three (approx.). Proportionally lower ripple can be achieved with higher capacitor values. Note that the capacitor will not affect operating frequency or efficiency, but it will increase start-up delay, by reducing the rate of rise of LED voltage.

By adding this capacitor the current waveform through the LED(s) changes from a triangular ramp to a more sinusoidal version without altering the mean current value .

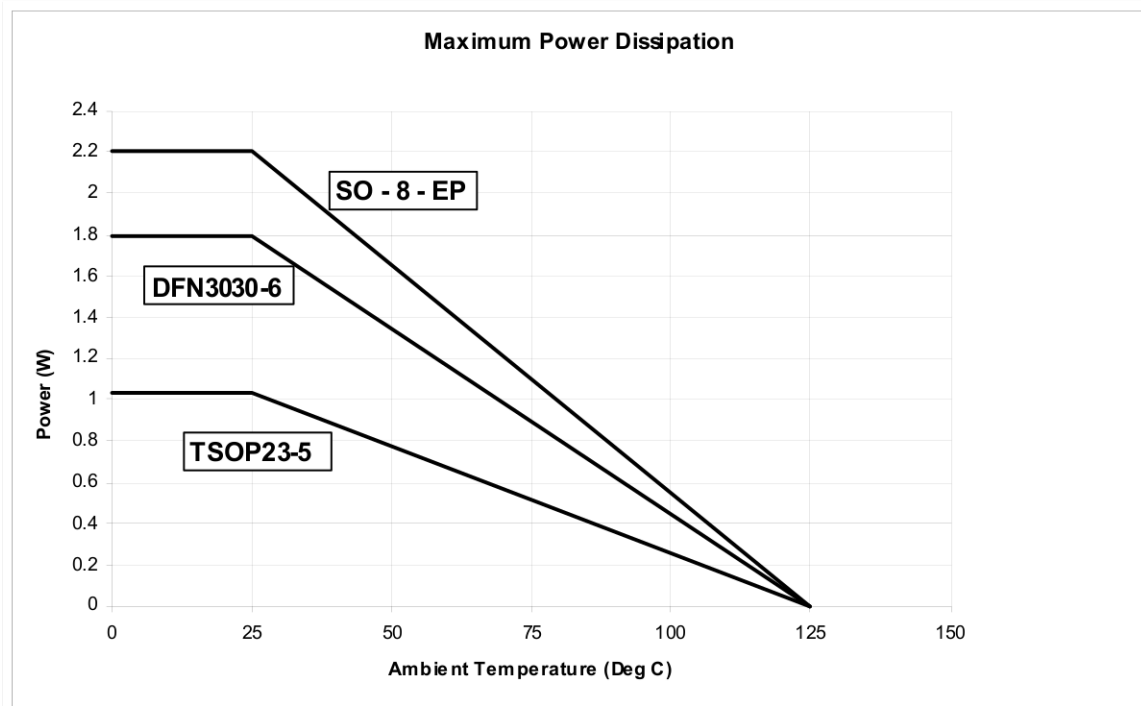
Operation at low supply voltage

Below the under-voltage lockout threshold (V_{SD}) the drive to the output transistor is turned off to prevent device operation with excessive on-resistance of the output transistor. The output transistor is not full enhanced until the supply voltage exceeds approximately 17V. At supply voltages between V_{SD} and 17V care must be taken to avoid excessive power dissipation due to the on-resistance.

Note that when driving loads of two or more LEDs, the forward drop will normally be sufficient to prevent the device from switching below approximately 6V. This will minimize the risk of damage to the device.

Thermal considerations

When operating the device at high ambient temperatures, or when driving maximum load current, care must be taken to avoid exceeding the package power dissipation limits. The graph below gives details for power derating. This assumes the device to be mounted on a 25mm² PCB with 1oz copper standing in still air.



Note that the device power dissipation will most often be a maximum at minimum supply voltage. It will also increase if the efficiency of the circuit is low. This may result from the use of unsuitable coils, or excessive parasitic output capacitance on the switch output.

In order to maximize the thermal capabilities of the DFN3030-6 and the SO-8-EP packages thermal vias should be incorporated into the PCB. See figures 7 and 8 for examples used in the ZXLD1366 evaluation boards.

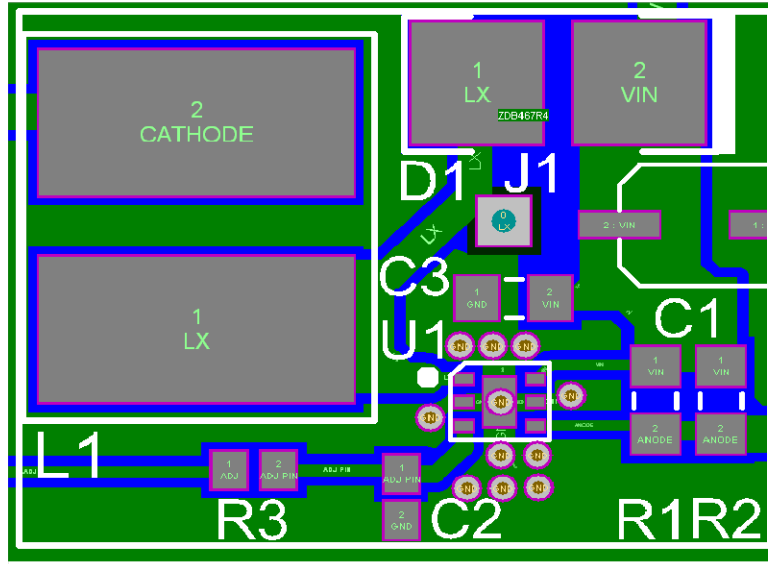


Figure 7 Suggested layout for DFN3030-6 package

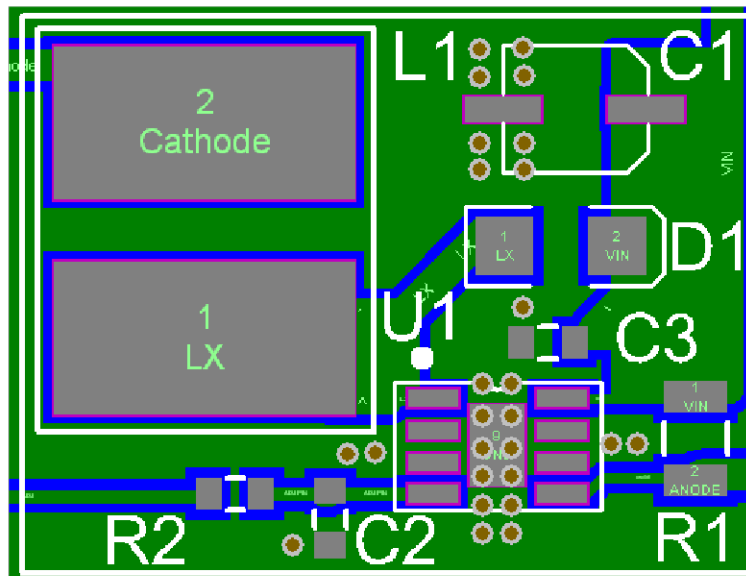


Figure 8 Suggested layout for SO-8-EP package

Vias ensure an effective path to the ground plane for the heat flow therefore reducing the thermal impedance between junction and ambient temperature. Diodes came to the conclusion that the compromise is reached by using more than 10 vias with 1mm of diameter and 0.5 hole size.

Finally the same scheme in figure 7 (without the exposed paddle) can be used for the TSOT23-5 package guaranteeing an effective thermal path.

Thermal compensation of output current

High luminance LEDs often need to be supplied with a temperature compensated current in order to maintain stable and reliable operation at all drive levels. The LEDs are usually mounted remotely from the device so, for this reason, the temperature coefficients of the internal circuits for the ZXLD1366 have been optimized to minimize the change in output current when no compensation is employed. If output current compensation is required, it is possible to use an external temperature sensing network - normally using Negative Temperature Coefficient (NTC) thermistors and/or diodes, mounted very close to the LED(s). The output of the sensing network can be used to drive the ADJ pin in order to reduce output current with increasing temperature.

Layout considerations

LX pin

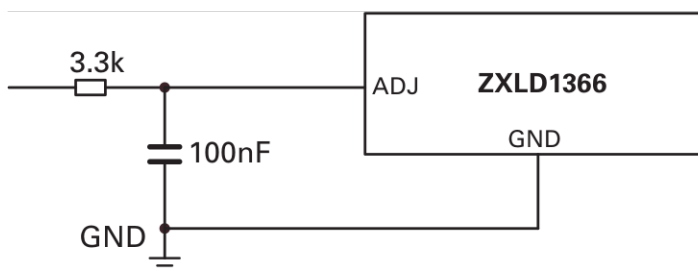
The LX pin of the device is a fast switching node, so PCB tracks should be kept as short as possible. To minimize ground 'bounce', the ground pin of the device should be soldered directly to the ground plane.

Coil and decoupling capacitors and current sense resistor

It is particularly important to mount the coil and the input decoupling capacitor as close to the device pins as possible to minimize parasitic resistance and inductance, which will degrade efficiency. It is also important to minimize any track resistance in series with current sense resistor R_S . Its best to connect V_{IN} directly to one end of R_S and I_{sense} directly to the opposite end of R_S with no other currents flowing in these tracks. It is important that the cathode current of the Schottky diode does not flow in a track between R_S and V_{IN} as this may give an apparent higher measure of current than is actual because of track resistance.

ADJ pin

The ADJ pin is a high impedance input for voltages up to 1.35V so, when left floating, PCB tracks to this pin should be as short as possible to reduce noise pickup. A 100nF capacitor from the ADJ pin to ground will reduce frequency modulation of the output under these conditions. An additional series 3.3k Ω resistor can also be used when driving the ADJ pin from an external circuit (see below). This resistor will provide filtering for low frequency noise and provide protection against high voltage transients.



High voltage tracks

Avoid running any high voltage tracks close to the ADJ pin, to reduce the risk of leakage currents due to board contamination. The ADJ pin is soft-clamped for voltages above 1.35V to desensitize it to leakage that might raise the ADJ pin voltage and cause excessive output current. However, a ground ring placed around the ADJ pin is recommended to minimize changes in output current under these conditions.

Evaluation PCB

ZXLD1366 evaluation boards are available on request. Terminals allow for interfacing to customers own LED products.

Dimming output current using PWM

Low frequency PWM mode

When the ADJ pin is driven with a low frequency PWM signal (eg 100Hz), with a high level voltage V_{ADJ} and a low level of zero, the output of the internal low pass filter will swing between 0V and V_{ADJ} , causing the input to the shutdown circuit to fall below its turn-off threshold (200mV nom) when the ADJ pin is low. This will cause the output current to be switched on and off at the PWM frequency, resulting in an average output current I_{OUTavg} proportional to the PWM duty cycle. (See Figure 4 - Low frequency PWM operating waveforms).

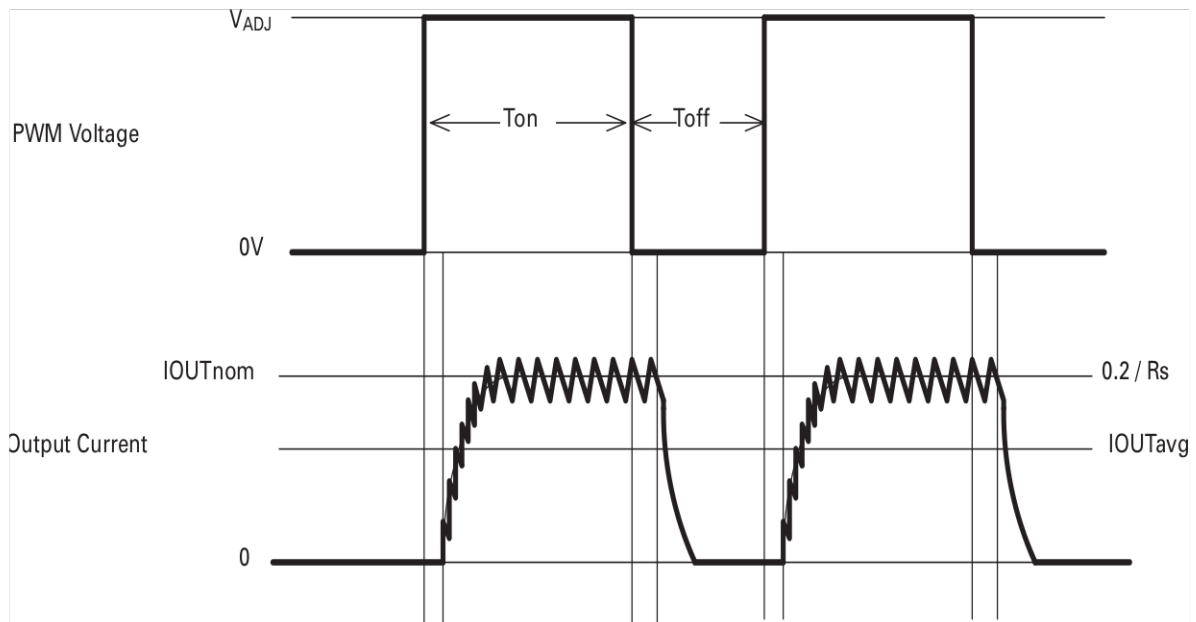


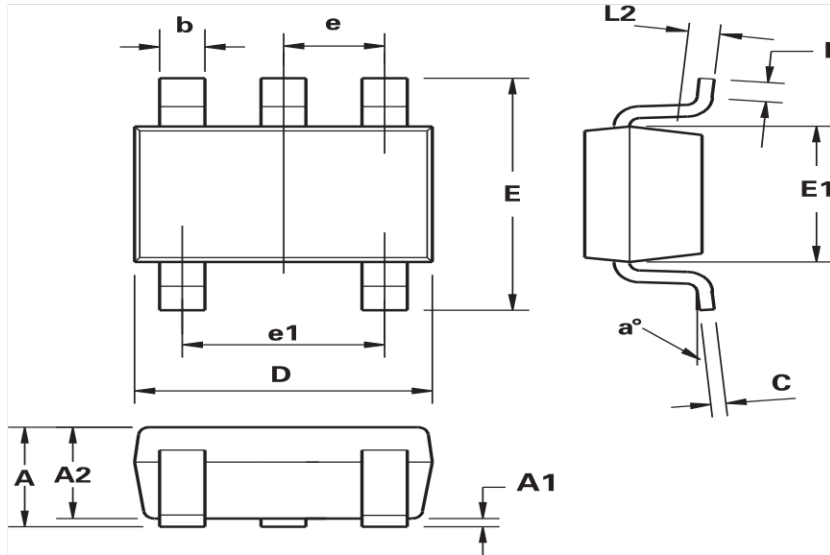
Figure 4 Low frequency PWM operating waveforms

The average value of output current in this mode is given by:

$$I_{OUTavg} = 0.2D_{PWM}/R_S \text{ [for } D_{PWM} > 0.001\text{]}$$

This mode is preferable if optimum LED 'whiteness' is required. It will also provide the widest possible dimming range (approx. 1000:1) and higher efficiency at the expense of greater output ripple.

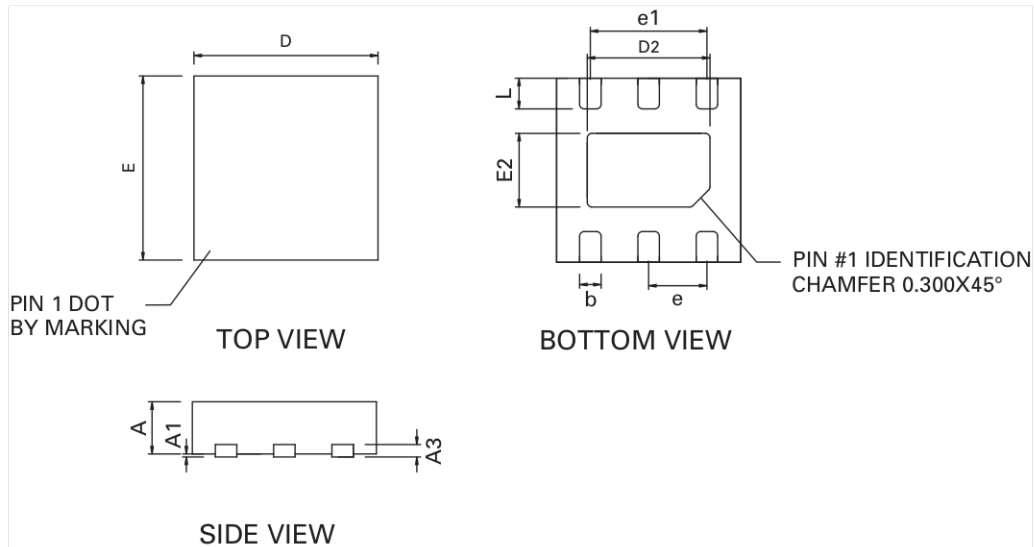
Package outline - TSOT23-5



DIM	Millimeters		Inches	
	Min.	Max.	Min.	Max.
A	-	1.00	-	0.0393
A1	0.01	0.10	0.0003	0.0039
A2	0.84	0.90	0.0330	0.0354
b	0.30	0.45	0.0118	0.0177
c	0.12	0.20	0.0047	0.0078
D	2.90 BSC		0.114 BSC	
E	2.80 BSC		0.110 BSC	
E1	1.60 BSC		0.062 BSC	
e	0.95 BSC		0.0374 BSC	
e1	1.90 BSC		0.0748 BSC	
L	0.30	0.50	0.0118	0.0196
L2	0.25 BSC		0.010 BSC	
a°	4°	12°	4°	12°

Note: Controlling dimensions are in millimeters. Approximate dimensions are provided in inches

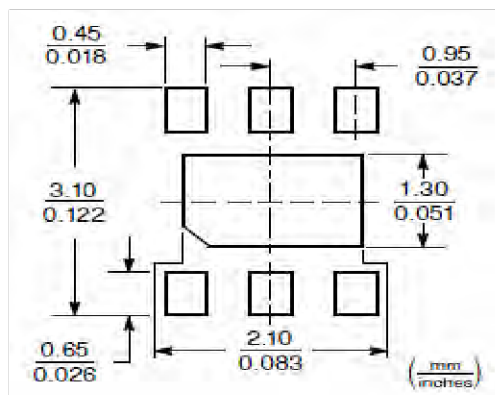
Package outline - DFN633



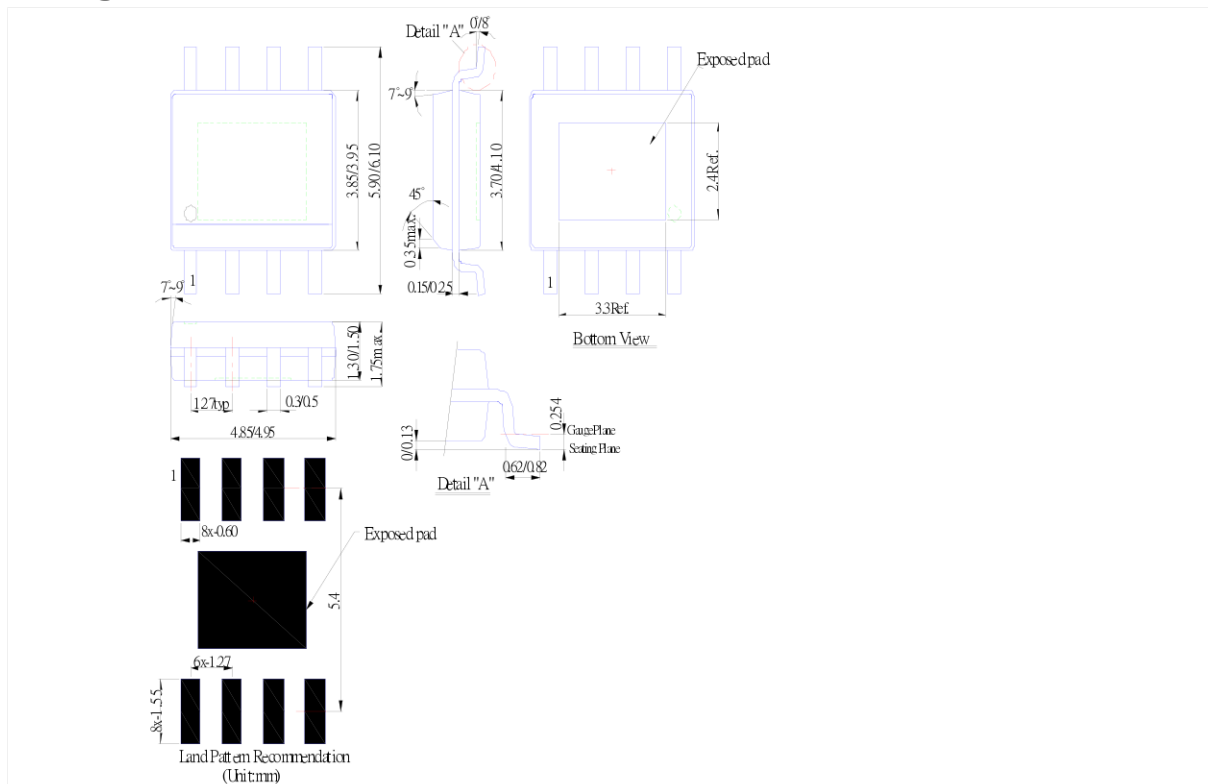
DIM	Millimeters		Inches		DIM	Millimeters		Inches	
	Min.	Max.	Min.	Max.		Min.	Max.	Min.	Max.
A	0.700	0.800	0.0275	0.0315	D2	1.950	2.050	0.0768	0.0807
A1	0.000	0.050	0.000	0.00197	e	0.950 BSC		0.0374 BSC	
A3	0.203 REF		0.008		E	2.950	3.050	0.116	0.120
b	0.300	0.400	0.0118	0.0157	E2	1.150	1.250	0.0452	0.0492
D	2.950	3.050	0.116	0.120	e1	1.900REF		0.0748	
					L	0.450	0.550	0.0177	0.0216

Note controlling dimensions in millimetres. Approximate dimensions are provided in inches

Solder/PCB Landing Pattern



Package outline - SO-8-EP



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